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Keywords: buck boost led driver, buck-boost, led driver

REFERENCE DESIGN 4452 INCLUDES: ✓Tested Circuit ✓Schematic ✓BOM ✓Board Available ✓Description ✓Test Data

Designing a Buck-Boost LED Driver Using the MAX16834

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Abstract: This reference design is for a buck-boost LED driver. The MAX16834 current-mode high-brightness LED driver is featured, and the MAX16834 EV (evaluation) kit is used to implement the design. The application note shows the design specifications, schematic, bill of materials (BOM), and performance data.

In this reference design a buck-boost converter (input-voltage referenced) drives 350mA through 4 white LEDs (WLEDs) from a 7V to 18V DC supply. The [MAX16834](#) current-mode high-brightness (HB) LED driver is featured.

LED Driver Specifications

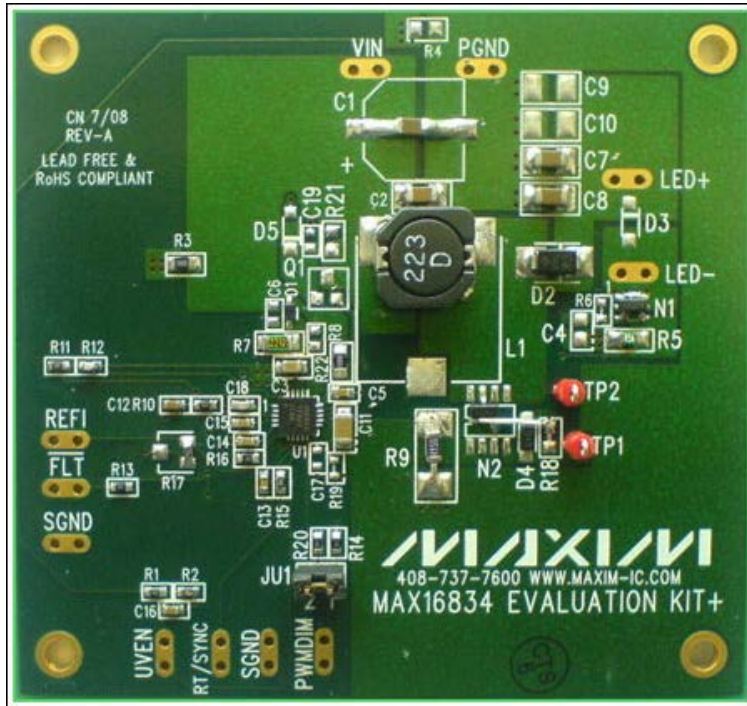
- Input voltage: 7V to 18V
- Input voltage ripple: 100mV_{P-P}
- LED current: 350mA
- LED current ripple: 5% (max)
- LED forward voltage: 3.5V at 350mA
- Number of LEDs: 4 (max)
- Output overvoltage protection: 17.2V

Inputs

- V_{IN} PGND: input supply voltage
- PWMDIM, SGND: input for PWM dimming

Outputs

- LED+: connect anode of LEDs to LED+
- LED-: connect cathode of LEDs to LED-



More detailed image (PDF, 60.64kB)

Figure 1. The MAX16834EVKIT was used to implement this reference design.

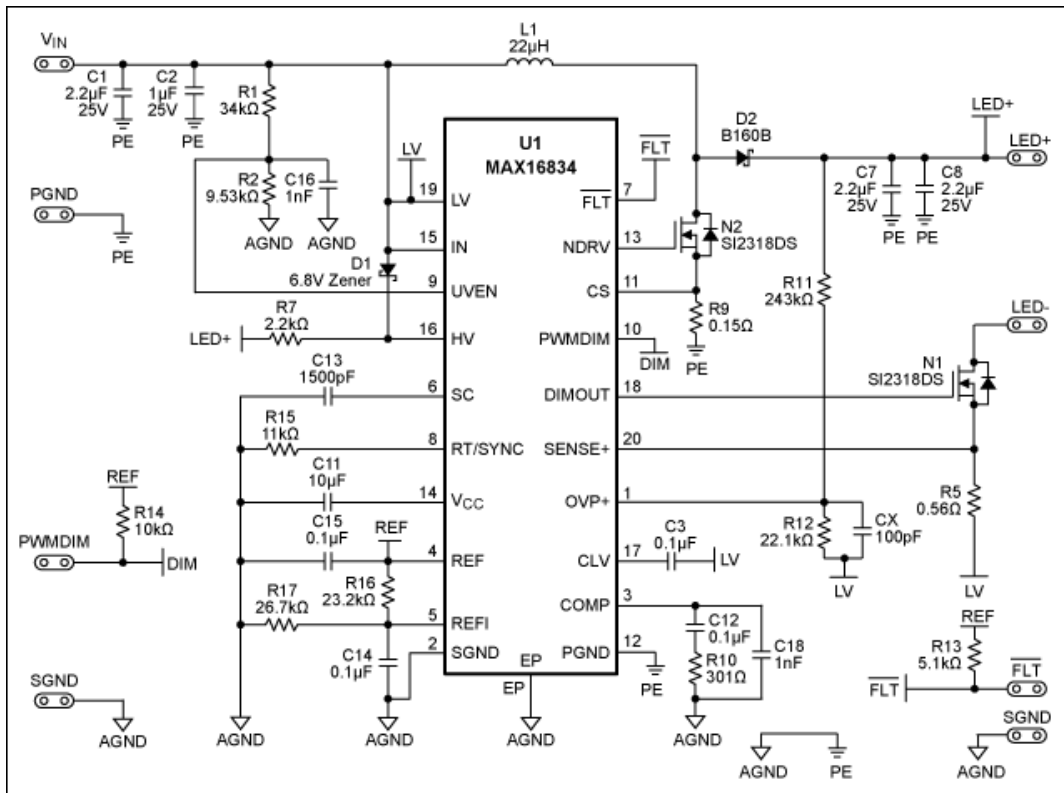


Figure 2. Schematic of the LED driver.

Component List* (Bill of Materials, BOM)

Ref	Part	Value	Notes
R1	Resistor	34kΩ	
R2	Resistor	9.53kΩ	
R3	Resistor	2.2kΩ	
R4	Resistor	2.2kΩ	
R5	Resistor	0.56Ω	
R6	Resistor	243kΩ	
R7	Resistor	2.2kΩ	
R8	Resistor	2.2kΩ	
R9	Resistor	0.15Ω	
R10	Resistor	301Ω	
R11	Resistor	243kΩ	
R12	Resistor	22.1kΩ	
R13	Resistor	5.1kΩ	
R14	Resistor	10kΩ	
R15	Resistor	11kΩ	
R16	Resistor	23.2kΩ	
R17	Resistor	26.7kΩ	

Designator	Quantity	Description
C1, C7, C8	3	2.2 μ F, 25V X7R, ceramic capacitor (0805)
C2	1	2.2 μ F, 25V X7R, ceramic capacitor (0805)
C11	1	10 μ F, 16V X7R, ceramic capacitor (1206)
C3, C12, C14, C15	4	0.1 μ F, 16V X7R, ceramic capacitor (0603)
C13	1	1.5nF, 10V X7R, ceramic capacitor (0603)
C16, C18	2	1nF, 10V X7R, ceramic capacitor (0603)
Cx	1	100pF, 10V X7R, ceramic capacitor (0603)
D1	1	MAZS0680ML, 6.8V Zener diode, SSMINI
D2	1	B160B, 1A, 60V Schottky diode
L1	1	MMS1038-223ML, 22 μ H, 2.34A inductor
N1, N2	2	SI2318DS, 40V, 3A, n-channel MOSFET (SOT23)
R1	1	34k Ω \pm 1% resistor (0402)
R2	1	9.53k Ω \pm 1% resistor (0402)
R7	1	2.2k Ω \pm 1% resistor (0805)
R5	1	0.56k Ω \pm 1% resistor (0803)
R9	1	0.15 Ω \pm 1% resistor (0603)
R10	1	310 Ω \pm 1% resistor (0402)
R11	1	243k Ω \pm 1% resistor (0402)
R12	1	22.1k Ω \pm 1% resistor (0402)
R13	1	13.1k Ω \pm 1% resistor (0402)
R14	1	10k Ω \pm % resistor (0402)
R15	1	11k Ω \pm 1% resistor (0402)
R16	1	23.2k Ω \pm 1% resistor (0402)
R17	1	26.7k Ω \pm 1% resistor (0402)
U1	1	MAX16834ATP+ 20-pin, 4mm x 4mm TQFN-EP

*Component designations match the MAX16834 EV kit board.

Detailed Description

Connecting the negative terminal of a boost converter's output to the input-positive supply results in a buck-boost converter (input-voltage referenced).

In this design a buck-boost converter (input-voltage referenced) drives 350mA through 4 white LEDs (WLEDs) from a 7V to 18V DC supply. (Each WLED has a forward voltage drop of 3.5V at 350mA.) The MAX16834 HB LED driver with integrated peak current-mode controller is used to design the converter, which operates in CCM (continuous conduction mode) at 495kHz switching frequency. The switching frequency is configured with the 11k Ω R15 resistor.

The MAX16834 controls the peak of the inductor current to achieve 350mA LED current under different input-output voltage conditions. The voltage across the LED current-sense resistor is sensed and then amplified by a factor of 9.9 internally. This results in a smaller value of sense resistor, thereby increasing the efficiency. This amplified voltage is then compared with the reference voltage set by resistors R16 and R17. The error is then amplified by the transconductance amplifier with $GM = 500\mu S$. This results in a control voltage across the COMP pin; this voltage sets the reference to the current loop. The peak of the voltage across the inductor current-sense resistor, R9, is tracked to this voltage.

Converter Design

The parameters for the converter design follow:

- Input supply-voltage range: 7V to 18V
- Input voltage ripple: 100mV_{P-P}
- Maximum LED forward voltage: 14V (which is 4 x 3.5V)
- LED current: 350mA
- LED current ripple: 5% (max)
- Switching frequency: 455kHz

Calculate the maximum duty cycle for N2 from Equation 1:

$$D_{MAX} = \frac{V_{LEDMAX} + V_D}{V_{INMIN} - V_{DS} + V_{LEDMAX} + V_D} \quad (\text{Eq. 1})$$

Where V_{LEDMAX} is the maximum LED voltage; V_{INMIN} is the minimum input voltage; V_D is the diode voltage drop; and V_{DS} is the average voltage across the FET when it is turned on.

In this application, D_{MAX} is 0.69.

Selecting the Inductor (L1)

To choose an inductor, both the inductor value and its peak current value must be known. Calculate the peak inductor current with Equation 2:

$$I_{LP} = I_{LAVG} \times (1 + \Delta I_L) \quad (\text{Eq. 2})$$

Where I_{LAVG} is the average inductor current. ΔI_L is the inductor current ripple, specified as the percentage of average inductor current:

$$I_{LAVG} = \frac{I_{LED}}{(1 - D_{MAX})} \quad (\text{Eq. 3})$$

Allow 30% ΔI_L . After substituting the known values, we get:

$$I_{LAVG} = 1.15A \text{ and } I_{LP} = 1.5A \quad (\text{Eq. 4})$$

Calculate the minimum inductance with Equation 5:

$$L_{MIN} = \frac{(V_{INMIN} - V_{DS}) \times D_{MAX}}{f_{SW} \times I_{LAVG} \times 2 \times \Delta I_L} \quad (\text{Eq. 5})$$

Where f_{SW} is the switching frequency. Allowing 20% tolerance results in $L_{MIN} = 17\mu H$. Here a $22\mu H$ inductor is chosen.

Switch Current-Sense Resistor (R9)

Under normal operating conditions the maximum voltage across the switch current-sense resistor must not be more than 250mV. If the sense-resistor voltage reaches 300mV (typ), then the converter is turned off. The voltage across R9 determines the ON pulse width of the switching cycle. Internal leading-edge blanking is provided to prevent premature turn-off of the switching MOSFET in a switching cycle. Calculate R9 with Equation 6:

$$R9 = \frac{0.25}{(1.25 \times I_{LP})} \quad (\text{Eq. 6})$$

Therefore, $R9 = 0.133\Omega$. Here a 0.15Ω resistor is chosen for R9.

Slope Compensation Capacitor (C13)

Peak current-mode control is known to be unstable at duty ratios more than 50% in a CCM boost-converter design. Proper slope compensation is, therefore, required to eliminate the instability caused by the subharmonic oscillations. The MAX16834 uses an internal ramp generator for slope compensation. The ramp resets at the beginning of each switching cycle and slews at the rate programmed by the external capacitor, C13. An internal $100\mu A$ current source charges this capacitor. This voltage is added to the voltage across R9 internally. Calculate the value of C13 with the Equation 7:

$$C13 = \frac{100\mu A}{V_{SLOPE}} \quad (\text{Eq. 7})$$

Where V_{SLOPE} is:

$$V_{SLOPE} = \frac{V_{LEDMAX} \times R9 \times 2}{L_{MIN} \times 3} \quad (\text{Eq. 8})$$

Therefore from Equations 7 and 8, $C13 = 1.57nF$. Here a $1.5nF$ capacitor is chosen.

LED Current-Sense Resistor (R5)

Calculate R5 with the Equation 9:

$$R5 = \frac{V_{REF1}}{(9.9 \times I_{LED})} \quad (\text{Eq. 9})$$

For this application V_{REF1} is selected as 1.94V. Therefore, $R5 = 0.56\Omega$.

Filter Capacitors

Calculate the value of output capacitor C_{OUT} (the parallel combination of C7 and C8) with Equation 10:

$$C_{OUT} = \frac{I_{LED} \times D_{MAX}}{f_{SW} \times \Delta V_{LED}} \quad (\text{Eq. 10})$$

Where ΔV_{LED} is the maximum peak-to-peak boost output-voltage ripple. This value depends on the maximum current ripple and the dynamic impedance of LEDs at the rated current. To prolong LED life and preserve chromaticity, the LED current ripple should be kept below 5% of the average current. In this application, C_{OUT} is calculated to be $3\mu\text{F}$. Accordingly, two capacitors of $2.2\mu\text{F}/50\text{V}$ each are chosen for C7 and C8.

Calculate the input capacitor value (the parallel combination of C1, C2) with Equation 11:

$$C_{IN} = \frac{I_{LAVG} \times \Delta I_L}{4 \times f_{SW} \times \Delta V_{IN}} \quad (\text{Eq. 11})$$

Where ΔV_{IN} is the peak-to-peak input voltage ripple.

For a 100mV ΔV_{IN} , C_{IN} is $1.9\mu\text{F}$. Therefore, C1 is selected as $2.2\mu\text{F}/25\text{V}$ and C2 as $1.1\mu\text{F}/25\text{V}$.

Feedback Compensation

A buck-boost converter, power-circuit transfer function has a right-half-plane zero calculated with Equation 12:

$$f_{RHPZ} = \frac{V_{LEDMAX} \times (1 - D_{MAX})^2}{2 \times \pi \times L_{MIN} \times I_{LED} \times D_{MAX}} \quad (\text{Eq. 12})$$

For this application, f_{RHPZ} occurs at 37.8kHz. To keep the feedback stable with sufficient phase margin, the total loop gain should cross 0dB before one-fifth of the RHP zero frequency at -20dB/decade. Thus the crossover frequency, f_C , is calculated to be 7.56kHz. The output capacitor and effective output impedance offered by the load create a pole at:

$$f_{P1} = \frac{1}{2 \times \pi \times R_O \times C_{OUT}} \quad (\text{Eq. 13})$$

Where R_O is the effective impedance contributed by the load, and is calculated as:

$$R_O = \frac{(R_{LED} + R5) \times V_{LEDMAX}}{(R_{LED} + R5) \times I_{LED} \times D_{MAX} + V_{LEDMAX}} \quad (\text{Eq. 14})$$

From Equation 14, $f_{P1} = 4.7\text{kHz}$.

Now the compensation components, R10 and C12, must be selected. They must contribute a zero at the pole frequency f_{P1} , and set the loop gain at f_{P1} so that loop gain crosses 0dB at f_C .

Calculate R10 with Equation 15:

$$R10 = \frac{f_C \times R9 \times [V_{LEDMAX} + (R_{LED} + R5) \times I_{LED} \times D_{MAX}]}{f_{P1} \times V_{LEDMAX} \times R5 \times (1 - D_{MAX}) \times 9.9 \times GM} \quad (\text{Eq. 15})$$

From Equation 15, $R10 = 341\Omega$. Here a 301Ω resistor is chosen for R10; GM is the gain of the internal transconductance amplifier.

Accordingly, C12 is calculated as:

$$C12 = \frac{1}{2 \times \pi \times R10 \times f_{p1}} \quad (\text{Eq. 16})$$

From Equation 16, C12 = 0.11µF. Here a 0.1µF capacitor is chosen.

Digital PWM Dimming

The MAX16834 has an internal PWM dimming MOSFET driver. PWM dimming is achieved by applying a 1.5V to 5V logic-high PWM signal with a frequency ranging from DC to 20kHz. The brightness of the LED can be varied by changing the duty ratio of the PWM signal.

The NDRV driver and the output of the transconductance amplifier are controlled by the PWM signal. When the PWM signal is high, then NDRV is enabled and the output of the transconductance amplifier is connected to the COMP pin. When the signal is low, NDRV is disabled and the output of the amplifier is disconnected. The COMP pin is connected to the negative input of the PWM comparator with CMOS inputs which draw negligible current from the compensation capacitor, C12. Thus the charge on C12 is preserved, thereby retaining the state when PWM was on. Once the signal becomes high, NDRV is enabled and the output of the amplifier is connected to the COMP pin. This establishes a steady-state operation quickly.

Open-LED Protection

The output of the boost converter can increase to high voltages, if it is operated without any load or if there is an open-LED fault. The converter can be disabled at a desired output voltage, which can be configured with the help of R11 and R12. The midpoint of R11 and R12 is connected to the OVP pin of the IC. The converter is disabled if the voltage across this pin reaches 1.435V (typ). In this application, R11 and R12 are configured to activate open-LED protection once the output voltage reaches 17.2V.

Implementation of the Buck Boost Converter on the MAX16834 EV Kit

The MAX16834 EV kit is assembled as a boost converter. The kit board can be reconfigured in buck-boost mode by removing and adding the following components:

- Remove resistors R4 and R8.
- Install a 0Ω resistor in place of R3.
- Install the components mentioned in the BOM.

Circuit Waveforms and Performance Data

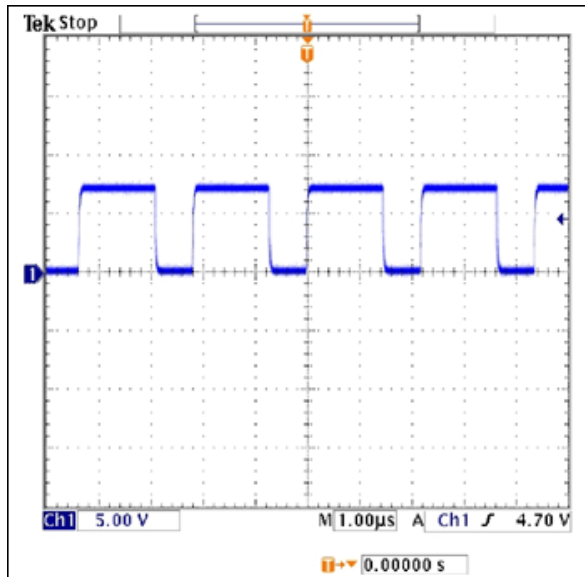


Figure 3. Gate driver voltage of N2.

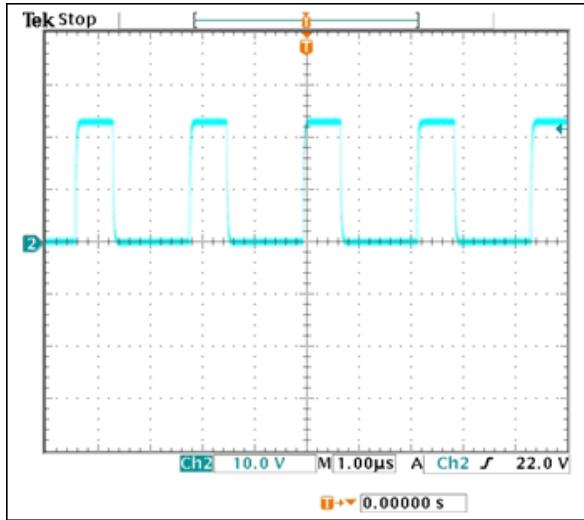


Figure 4. Drain voltage of N2.

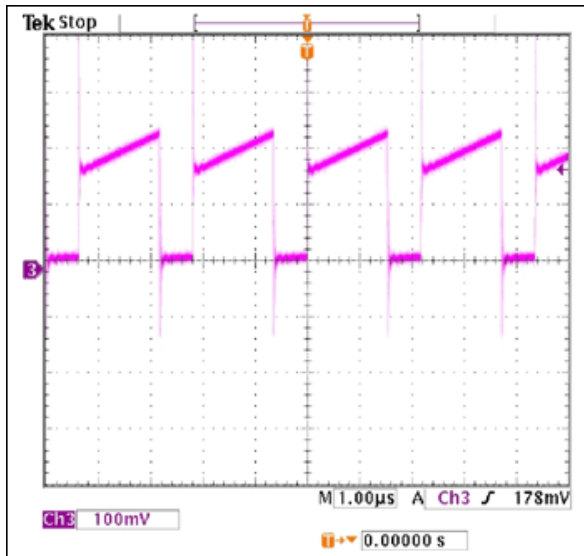


Figure 5. Switch current waveform of N2.

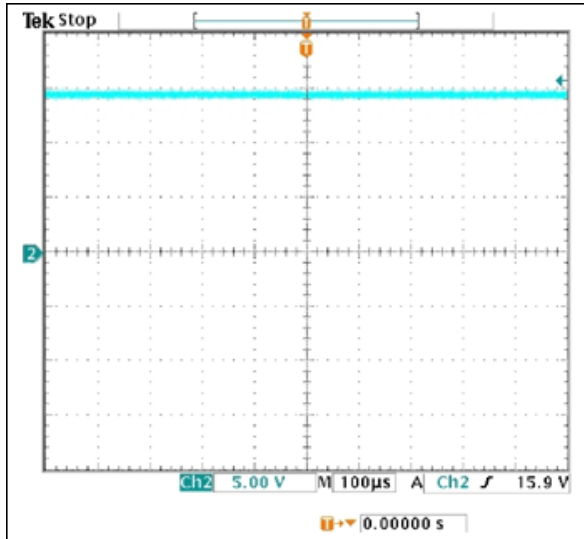


Figure 6. LED voltage.

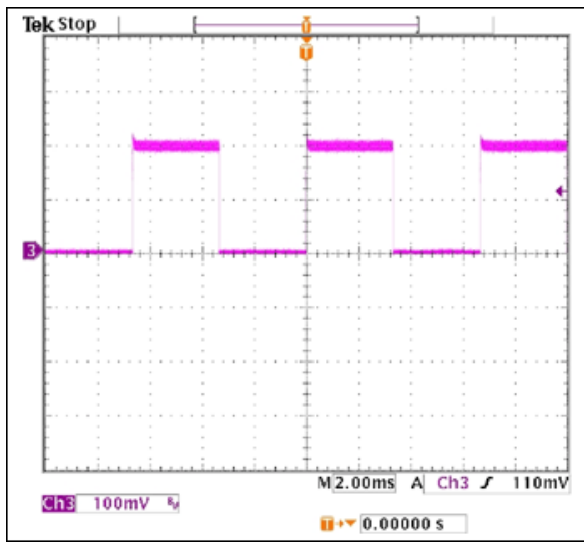


Figure 7. LED current waveform at 50% PWM dimming.

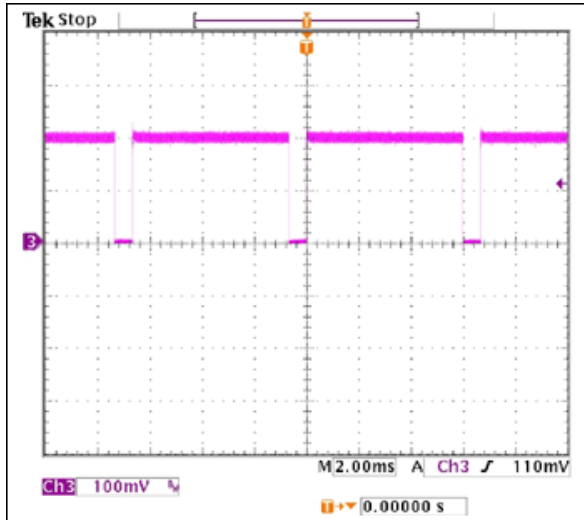


Figure 8. LED current waveform at 90% PWM dimming.

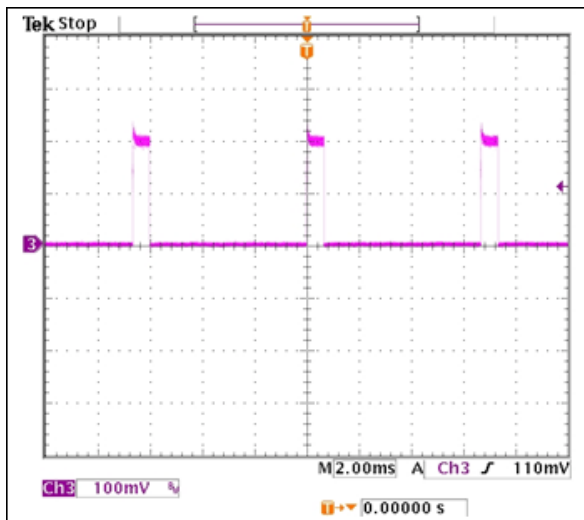


Figure 9. LED current waveform at 10% PWM dimming.

Power-Up Procedure

- Connect the string of 4 WLEDs with anode connected to the LED+ pad and cathode to the LED- pad.
- Connect the input power-supply input across the V_{IN} and PGND pads.
- Apply a 1.5V to 5V logic-high PWM signal with a frequency ranging from 100Hz to 200kHz across the PWMDIM and SGND pads.
- To vary the brightness of LEDs, vary the PWM signal duty ratio.

Related Parts

[MAX16834](#)

High-Power LED Driver with Integrated High-Side LED Current Sense and PWM Dimming MOSFET Driver

[Free Samples](#)

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